WDM/FDM STAR COUPLER WITH GAIN USING FIBRE AMPLIFIERS

Y.-K. Chen* and S. Chi

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An efficient amplified WDM/FDM star coupler is proposed. The size of the coupler can be increased by a factor of m using m fibre amplifiers. Furthermore, the complexity and cost of the proposed scheme are less than those of other configurations.

Introduction: Large N x N fibre-optic star couplers can be quite useful for high-throughput multiple-access WDM networks [1]. However, its inherent 1/N splitting loss may limit the ultimate size of the star coupler. Potential use of erbium-doped fibre (EDF) amplifiers to increase the number of users that a fibre-optic star network can support has been investigated by many researchers [2-4]. Both configurations in References 1 and 2 have the disadvantage that each receiver would require its own EDF amplifier, which can be quite expensive. The main advantage of the configuration in Reference 3 is a lower number of required EDF amplifiers and pump lasers than that of References 2 and 3. However, more components such as m different wavelength-dedicated bandpass filters (BPFs) and bandstop filters (BSFs) are necessary to control the operation of the m(N - 1) x m(N - 1) star coupler in Reference 4, and special requirements of m EDF amplifiers with high output saturation power level are necessary to overcome the problem of multiple communication links between different nodes of the network. In this Letter, we propose a novel technique to overcome these aforementioned problems.

Configuration and characteristics: A new configuration for the proposed mN x mN star coupler is shown in Fig. 1. It is composed of mN x 1 singlemode WDM multiplexers, one (m + 1) x (m + 1) passive star coupler, m EDF amplifiers pumped with a single pump laser, and m x N tree couplers. In fully transparent WDM/FDM star networks, each user is transmitting its information on a fixed unique wavelength.

Therefore, for the mN users supported by this network, mN wavelengths and m different multiplexers are needed. For each multiplexer, N users are directly connected via fibre links to its N input ports and its output port is connected to an EDF whose output is connected to one of the input ports of the (m + 1) x (m + 1) coupler; each output port of the (m + 1) x (m + 1) coupler is connected to a 1 x N tree coupler. The remaining output port of the (m + 1) x (m + 1) passive coupler is used to couple the pump laser light and distribute it equally among the EDF amplifier using a backward pumping scheme.

If mN users are distributed uniformly around a circle of diameter D over mN locations, then the number of standard fibres required to interconnect these mN users is 2. mN. A total fibre length of mN.D and total conduit length of mN.D/2 are needed to implement this star network. The link attenuation, L_T [dB], between any two users in this centralised star network shown in Fig. 1 is

\[ L_T = 10 \log (L_{MUX}) + 10 \log [(m + 1) \times N] + 10 \log (L_{F1}) + 10 \log (s_p \times D) \]

where \( L_{MUX} \) is the insertion loss of each WDM multiplexer, \( L_{F1} \) is the total excess loss of the (m + 1) x (m + 1) coupler, \( s_p \) is the fibre loss per unit length, and \( s_F \) is the fibre loss per unit length. Although \( L_T \) is \( L(1.2 \text{~mm}) \) larger than that of the configuration in Reference 4, these WDM multiplexers employ a diffraction grating design and can achieve channel spacing of the order of 1-2 nm such that they can accommodate 40-50 channels with an excess loss of \( \approx 7 \text{~dB} \) per channel [5].

The EDF amplifier with its wide gain profile is suitable for WDM/FDM systems due to its comparatively long gain recovery time, which makes the EDF amplifier immune to the intersymbol interference crosstalk effects over a wide range of bit rates [6]. In the broadcast operation mode, assume the signal gain of each EDF amplifier is the same, then the net gain from one user to another is 10 log (G - \( L_T \) [dB]), which is the same for all users. Therefore, the problem of variations of received signal due to multiple communication links between different nodes in Reference 4 is alleviated without using m different BPFs and BSFs. Besides the saving of these wavelength-dedicated BPFs and BSFs, it is found that the number of supportable users by the network of this proposed coupler is m larger than that of the other proposed mN - 1) x m(N - 1) star coupler in Reference 4.

Distributed configuration: In many practical networks, users are geographically distributed in many clusters. Hence, it is better to distribute the components of the centralised star coupler over several nodes to reduce the total fibre length and conduit length as compared with the centralised star network [7, 8]. The proposed configuration in Fig. 1 can easily be modified to form a distributed configuration as shown in Fig. 2.
2. Except for the physical separation between its components, this distributed coupler is itself a star network and is identical to the original centralised network and therefore will exhibit the same performance. In general, if mN users are distributed uniformly around a circle of diameter D over m nodes, then the total fibre length and conduit length are mD and mD/2, respectively, which are 1/N and 1/N of those required for the centralised case. Hence, the total fibre length and conduit length required for the distributed star network can be reduced greatly; this further increases the cost effectiveness significantly.

Conclusions: We have proposed a new technique, by which the size of a star coupler in WDM/FDM star networks can be increased m times by using m fibre amplifiers. The complexity and cost of the proposed scheme are so far over than those of other configurations. Furthermore, the required total fibre length and conduit length can be greatly reduced for the distributed configuration, thereby significantly increasing cost effectiveness.

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Y.-K. Chen* and S. Chi (Institute of Electro-Optical Engineering and Center for Telecommunications Research, National Chiao-Tung University, Hsinchu, Taiwan, Republic of China)

* Also with Telecommunication Laboratories, Ministry of Transportation and Communications, Republic of China

References

R-MOSFET STRUCTURE BASED ON CURRENT DIVISION

K. Vavalidis and Y. Tsividis

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A parallel-path combination of resistors and MOSFETs is proposed for use in integrated continuous-time filters and other circuits. The technique allows continuous incremental tuning while maintaining significantly better linearity than MOSFET-only structures.

Introduction: High-linearity integrated continuous-time filters employ linear resistors and capacitors. To compensate for tolerances and environmental changes, switchable element arrays are used [1, 2]. The resulting quantised tuning imposes a limit on tuning accuracy (e.g. to ±5%) and can cause disturbances in the output during tuning. If MOSFETs are used in lieu of resistors, a continuous tuning range becomes possible; however, even using special nonlinearity cancellation techniques [3-5], significant distortion is present (typically -60dB for 1 V peak to peak signals). To achieve a compromise, we can use combinations of resistors and MOSFETs [6, 7] which are based on voltage division across the latter for distortion reduction (compared to the MOSFET-only case). However, these need extra active elements [6] or introduce extra nodes [7] which, at high frequencies, can become vulnerable to parasitic capacitances. In this Letter, we propose an R-MOSFET technique which is instead based on current division, in a manner similar to that used with transconductors [8]; contrary to the latter case, though, here no complicated transconductor circuits need to be designed.

Principle of operation: The proposed scheme is shown in Fig. 1. The boxes in the feedback loop can be capacitors (for an integrator) or resistors (for an amplifier). Some elements in Fig. 1 can belong to switchable arrays for coarse tuning. Block X accomplishes fine tuning; in this block, four identical

MOSFETs are operated resistively in the triode region of operation and their nonlinearities cancel out [4, 5]. The circuit is designed so that the differential current \( I_x - I_y \) is a small fraction \( \eta \) of the resistor current \( I_R - I_L \). The voltages \( V_{C1}, V_{C2} \) are tuning voltages and \( V_{CM} \) is a common-mode voltage. In the following, by 'conductance' we mean the ratio of the linear part of the differential output current to the differential input voltage, 2\( V_{CM} \). The effective conductance of block X is [4, 5]

\[
G_x = \frac{\mu C_{ox}}{L}(V_{C1} - V_{C2})
\]

where the symbols have their usual meaning. Normally \( V_{C1} \neq V_{C2} \) and the effective conductance of the entire combination is \( G_0 \). By making \( V_{C1} = V_{C2} \), the effective conductance can be tuned by the factor \((1 + \eta)\), where

\[
\eta = \frac{G_x}{G_0}
\]

and \( \eta \) can be made positive or negative as seen from eqn. 1.

Distortion: Let \( I_{AX} \) be the residual nonlinear component in \( I_x - I_y \) due to second-order effects and mismatches [4]. The same component appears in the total differential \( I - I' \), which, however, contains in addition the much larger linear component \( I_R - I_L \); the fractional nonlinearity in \( I - I' \) is improved, compared to that in \( I_x - I_y \), by a factor of approximately \( \eta \).

Thus for any distortion measure (harmonic distortion, intermodulation distortion, etc.) we have

\[
D \approx \eta D_x
\]

where \( D \) refers to the combined structure, and \( D_x \) to block X. If this performance is not adequate, we can consider replacing